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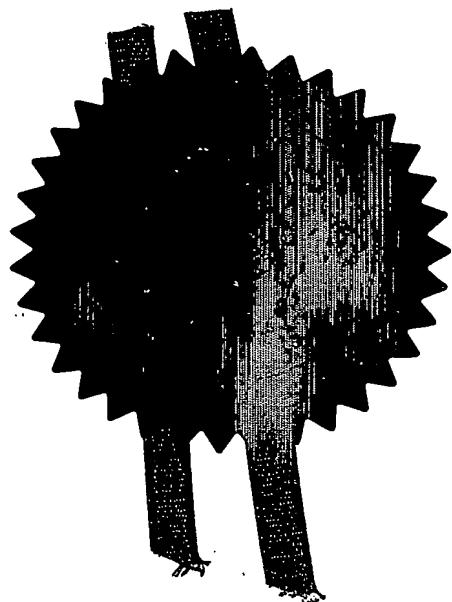
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Your reference

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Patent application number
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Full name, address and postcode of the or of each applicant (underline all surnames)

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00615336004
Patents ADP number (if you know it)

08281107001

If the applicant is a corporate body, give the country/state of its incorporation

U.S.A.

DELAWARE

Title of the invention

A DECODER FOR A WIRELESS COMMUNICATION DEVICE

Name of your agent (if you have one)

CHRISTOPHER HARRISON

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Patents ADP number (if you know it)

07957749001

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Country

Priority application number
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Signature

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12/1/2003

12. Name and daytime telephone number of person to contact in the United Kingdom

CHRISTOPHER HARRISON

Eliza LAURIE

01256-790763

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DUPLICATE

5

A DECODER FOR A WIRELESS COMMUNICATION DEVICE

The present invention relates to a decoder for a wireless communication device.

10 Wireless communication systems are widely deployed to provide various types of communications such as voice and data. One such system is wideband code division multiple access WCDMA, which has been adopted in various competing wireless communication standards, for example 3rd generation partnership project 3GPP and 3GPP2.

15 To overcome data corruption that can occur during RF transmission the different wireless communication standards typically include some form of channel coding, where one common channel coding technique is turbo coding.

20 Turbo coding involves the use of a turbo encoder for encoding a code segment (i.e. a data packet) and a turbo decoder for the decoding of the encoded code segment.

25 A turbo encoder includes two convolutional encoders and an interleaver, where the interleaver shuffles (i.e. interleaves) the information bits in the packet in accordance with a specified interleaving scheme.

30 The turbo encoder uses a first convolutional encoder to encode information bits within a packet to generate a first sequence of parity bits in parallel to the interleaver shuffling the information bits, where the shuffled information bits are encoded by a second encoder to generate a second sequence of parity bits. The information bits and the parity bits in the first and second sequence are then modulated and transmitted to a receiver.

5

The information bits and the first and second sequence of parity bits are received by a receiver and decoded by a turbo decoder.

10 The turbo decoder initially stores the received information bits and the parity bits in the first and second sequence in a buffer. Initially, the information bits and the first sequence of parity bits from the first convolutional encoder are retrieved from the buffer and decoded by a first soft input soft output SISO decoder to provide 'extrinsic' information indicative of adjustments in the confidence in the detected values for the information bits. Intermediate results that include the 15 extrinsic information from the first SISO decoder are then stored in the buffer in an interleaved order matching the code interleaving used at the transmitter.

20 The intermediate results, the information bits and the second sequence of parity bits from the second encoder are retrieved from the buffer and decoded by a second SISO decoder to provide extrinsic information indicative of further adjustments in the confidence in the detected values for the information bits. Intermediate results that comprise the extrinsic information from the second SISO decoder are then stored in the buffer in a deinterleaved order complementary to the code interleaving performed at the transmitter. The intermediate results are 25 used in a next decoding iteration performed by the turbo decoder. The turbo decoder performs a predetermined number of decoding iterations before producing a decision on the value of the decoded information bit.

30 Commonly used algorithms used within SISO decoders are the maximum a posteriori MAP decoding algorithm and the log MAP decoding algorithm. The log MAP decoding algorithm is analogous to the MAP decoding algorithm but performed in the logarithmic domain.

5 The MAP decoding algorithm uses forward state metrics, commonly referred to as alphas α , and backward state metrics, commonly referred to as betas β , to determine soft output results, where the forward state metrics α and backward state metrics β characterise a state in a trellis structure.

10 The MAX* function is used within the log-MAP algorithm and is represented by $\text{MAX}^*(\alpha(n), \beta(n))$, where $\alpha(n)$ and $\beta(n)$ are inputs to the MAX* function. The inputs $\alpha(n)$ and $\beta(n)$ can be forward state metrics, backward state metrics or a combination of both.

15 The $\text{MAX}^*(\alpha(n), \beta(n))$ function is equal to $\text{MAX}(\alpha(n), \beta(n))$ plus a correction value where the correction value is equal to $\log(1+\exp(-|\alpha(n) - \beta(n)|))$.

20 The $\text{MAX}(\alpha(n), \beta(n))$ term of the equation is usually straight forward to calculate, however the correction value is relatively complicated to calculate and is usually approximated using either a linear approximation, a step approximation or a look-up table.

25 As the state metric calculations are performed within the SISO decoder the values within the accumulated path metrics can overflow leading to incorrect results.

30 One solution to the overflow problem involves the use of modulo arithmetic's. A modulo n operation on a number provides the remainder when the number is divided by n , for example $10(\text{binary } 1010) \bmod 8 = 2(\text{binary } 010)$ and $28(\text{binary } 11100) \bmod 16 = 12(\text{binary } 1100)$. Consequently, as can be seen from the examples, determine a value for a modulo operation where the remainder is a value to the power of two is simply a question of masking off any unwanted bits.

5 The modulo function, as illustrated in figure 1, can be regarded as a sawtooth function.

An alternative implementation of the modulo function can be defined by:
$$xmodF = x - 2F \left\lfloor \left(\frac{x+F}{2F} \right) \right\rfloor$$
, which allows negative numbers to be accommodated.

10 This function is illustrated in figure 2.

It is desirable to have an apparatus and method for generating a linearly approximated MAX* log MAP algorithm that operates on modulo functions.

15 In accordance with a first aspect of the present invention there is provided a decoder for a wireless communication device according to claim 1.

In accordance with a second aspect of the present invention there is provided a method for generating a MAX* value according to claim 8.

20

An embodiment of the invention will now be described, by way of example, with reference to the drawings, of which:

Figure 1 illustrates a graphical representation of a first modulo function;

25

Figure 2 illustrates a graphical representation of a second modulo function;

Figure 3 illustrates a graphical representation of the variation in the MAX* correction term versus $|a(n) - b(n)|$;

30

5

Figure 4 illustrates a decoder according to an embodiment of the present invention.

The curve A in figure 3 illustrates the correction term for the $\text{MAX}^*(a(n), b(n))$ function (i.e. $\text{MAX}^*(a(n), b(n)) - \text{MAX}(a(n), b(n))$) as a function of $|a(n) - b(n)|$, where 10 $|a(n) - b(n)|$ is the absolute value of the difference between $a(n)$ and $b(n)$.

As can be seen from curve A the correction term is greatest for low values of $|a(n) - b(n)|$ and gradually decreases to zero as $|a(n) - b(n)|$ increases.

1.5 As stated above, an easy technique for approximating the correction term is the use of linear approximation, as illustrated by line B in figure 3. As illustrated, the linear approximation provides a close approximation for the correction term for low values of $|a(n) - b(n)|$. The intersection of the line B on the $|a(n) - b(n)|$ axis indicates the $|a(n) - b(n)|$ value above which the linear approximation correction 20 term goes to zero. Consequently, using linear approximation, the intersection point determines a threshold value, designated C, for determining if a correction value is to be applied to $|a(n) - b(n)|$, where the intersection point is defined by the linear approximation equation.

25 The use of the linear approximation technique allows easy calculation of the MAX^* function, as described below.

One suitable linear approximation equation (i.e. the correction term used) is given by $\text{MAX}(0, \frac{(C - |a(n) - b(n)|)}{2})$.

30

Consequently, the MAX^* function can be written as:

5 $\text{MAX}(a(n), b(n)) + \text{MAX}(0, \frac{(C - |a(n) - b(n)|)}{2})$

$$= \text{MAX}(0 + \text{MAX}(a(n), b(n)), \frac{(C - |a(n) - b(n)|)}{2} + \text{MAX}(a(n), b(n)))$$

$$= \text{MAX}(a(n), b(n), \frac{(a(n) + b(n) + C)}{2} + \text{MAX}(a(n), b(n)))$$

10

$$= \text{MAX}(a(n), b(n), \frac{(a(n) + b(n) + C)}{2})$$

15 To minimise the problem of accumulated state metric overflow, as discussed above, the above terms are converted into their corresponding 'modF' values where F is selected such that $|a(n) - b(n)| < F$. F is chosen by analysing the algorithm and determining what would be the maximum possible value of $|a(n) - b(n)|$ for any $a(n)$ and $b(n)$ that can enter the MAX^* function.

20 To ease the hardware implementation for handling the modulo value F is preferable a value to the power of two.

The modF of $a(n)$ becomes $a(n)\text{mod}F$.

The modF of $b(n)$ becomes $b(n)\text{mod}F$.

25

However, the modF of $(a(n) + b(n) + C)/2$ is

$$\left(a(n)\text{mod}F + \frac{(b(n)\text{mod}F - a(n)\text{mod}F)\text{mod}F + C}{2} \right) \text{mod}F$$



5

and not $\left(\frac{a(n) \bmod F + b(n) \bmod F + C}{2} \right) \bmod F$.

This is demonstrated by the following:

The equation $x \bmod F$ is equivalent to $x - 2F \left\lfloor \left(\frac{x+F}{2F} \right) \right\rfloor$, where the $\lfloor x \rfloor$ term is

10 the floor of 'x'.

Accordingly:

$$(a(n)+C) \bmod F = (a(n) \bmod F + C) \bmod F$$

15 and

$$(a(n)-b(n)) \bmod F = a(n) - b(n) \text{ if and only if } |a(n) - b(n)| < F$$

Using these two identities proves:

$$20 \quad \left(\frac{a(n) + b(n) + C}{2} \right) \bmod F = \left(a(n) + \left(\frac{b(n) - a(n) + C}{2} \right) \right) \bmod F$$

$$= \left(a(n) \bmod F + \left(\frac{(b(n) - a(n)) \bmod F + C}{2} \right) \right) \bmod F$$

$$= \left(a(n) \bmod F + \frac{((b(n) \bmod F - a(n) \bmod F) \bmod F + C)}{2} \right) \bmod F$$

25

5 For values of $C < F/2$ an alternative implementation of the modulo of a linear approximation of a MAX function is equal to:

$$\left(\left(\frac{(a(n) \bmod F + C) \bmod F + b(n) \bmod F}{2} \right) \bmod F + F * s \right) \bmod F$$

10 where s is calculated from the binary expression $s = [a(m) \text{ xor } b(m)]$ and $[(a(m) \text{ xor } a(m-1)) \text{ and } ((b(m) \text{ xor } b(m-1))]$, where a and b are represented by m bits so that $a(m)$ is the most significant bit of a and $a(m-1)$ is next to the most significant bit.

15 This algorithm is easy to calculate in silicon as s involves only binary operations and F is chosen to be a power of two.

20 A decoder 400 for implementing the above MAX* equation is shown in figure 4 and is arranged to output $\text{MAX}(a(n) \bmod F, b(n) \bmod F)$ when $|a(n) - b(n)|$ is greater than the threshold value C and to output $\left(a(n) \bmod F + \frac{((b(n) \bmod F - a(n) \bmod F) \bmod F + C)}{2} \right) \bmod F$ when $|a(n) - b(n)|$ is less than the threshold value C . If $|a(n) - b(n)|$ equals C then either $\text{MAX}(a(n) \bmod F, b(n) \bmod F)$ or

$$\left(a(n) \bmod F + \frac{((b(n) \bmod F - a(n) \bmod F) \bmod F + C)}{2} \right) \bmod F \text{ can be output.}$$

25 The decoder 400 includes a first subtracting unit 401, a second subtracting unit 402, a calculator 403 in the form of an adder unit and a selector 404 in the form of a multiplexer unit. The first subtracting unit 401, the

5 second subtracting unit 402 and the adder unit 403 are each arranged to receive $a(n)modF$, $b(n)modF$ and the threshold value C.

10 The first subtracting unit 401 is arranged to generate the sign of $(b(n)modF - a(n)modF - C)modF$. The second subtracting unit 402 is arranged to generate the sign of $(a(n)modF - b(n)modF - C)modF$. The adder unit 403 is arranged to generate $\left(a(n)modF + \frac{((b(n)modF - a(n)modF)modF + C)}{2} \right)modF$, where the division by two corresponds to a shift in bit position by one.

15 The modF operation is performed by ignoring the overflow (i.e. the carry bit of the msb bit addition is ignored).

20 The output from the first subtracting unit 401, the second subtracting unit 402 and the adding unit 403 (i.e. the sign of $(b(n)modF - a(n)modF - C)modF$, the sign of $(a(n)modF - b(n)modF - C)modF$ and $\left(a(n)modF + \frac{((b(n)modF - a(n)modF)modF + C)}{2} \right)modF$ respectively) are provided to the multiplex unit 404 along with the values of $a(n)modF$ and $b(n)modF$.

25 The multiplexer 404 is arranged to output a $\text{MAX}^*(a(n)modF, b(n)modF)$ equal to $a(n)modF$ when the sign of $(a(n)modF - b(n)modF - C)modF$ is positive and the sign of $(b(n)modF - a(n)modF - C)modF$ is negative.

5 The multiplexer 404 is arranged to output a $\text{MAX}^*(a(n)\text{mod}F, b(n)\text{mod}F)$ equal to $b(n)\text{mod}F$ when the sign of $(a(n)\text{mod}F-b(n)\text{mod}F-C)\text{mod}F$ is negative and the sign of $(b(n)\text{mod}F-a(n)\text{mod}F-C)\text{mod}F$ is positive.

10 The multiplexer 404 is arranged to output a $\text{MAX}^*(a(n)\text{mod}F, b(n)\text{mod}F)$ equal to $\left(a(n)\text{mod}F + \frac{((b(n)\text{mod}F - a(n)\text{mod}F)\text{mod}F + C)}{2}\right)\text{mod}F$ when the sign of $(a(n)\text{mod}F-b(n)\text{mod}F-C)\text{mod}F$ is negative and the sign of $(b(n)\text{mod}F-a(n)\text{mod}F-C)\text{mod}F$ is negative.

15 It will be apparent to those skilled in the art that the disclosed subject matter may be modified in numerous ways and may assume many embodiments other than the preferred forms specifically set out as described above, for example the above embodiments could be arranged such that the modulo for other linear approximation equations can be calculated and an additional subtracting unit could be used to determine the sign of $a(n)-b(n)$ to assist the selection process.

CLAIMS

1. A decoder for a wireless communication device comprising a calculator for calculating the modulo of a linear approximation of a MAX* function; and a selector for selecting a MAX* output value from the group $a(n) \bmod F$, $b(n) \bmod F$, and the calculated modulo based upon a determination as to whether a predetermined threshold value for $|a(n) - b(n)|$ has been met, where $a(n)$ is a first state metric, $b(n)$ is a second state metric, C is the predetermined threshold value and F is a value greater than $|a(n) - b(n)|$.
10
2. A decoder according to claim 1, wherein the calculator is arranged to calculate the modulo of a linear approximation of a MAX function using:
$$\left(a(n) \bmod F + \frac{((b(n) \bmod F - a(n) \bmod F) \bmod F + C)}{2} \right) \bmod F.$$

15
3. A decoder according to claim 1, wherein the calculator is arranged to calculate the modulo of a linear approximation of a MAX function using:
20
$$\left(\left(\frac{(a(n) \bmod F + C) \bmod F + b(n) \bmod F}{2} \right) \bmod F + F * s \right) \bmod F, \text{ where } s \text{ is equal to } [a(m) \bmod F \text{ xor } b(m) \bmod F] \text{ and } [((a(m) \bmod F \text{ xor } a(m-1)) \bmod F \text{ xor } (b(m) \bmod F \text{ xor } b(m-1)) \bmod F]$$
4. A decoder according to claim any preceding claim, wherein the determination is based upon the sign of $(a(n) \bmod F - b(n) \bmod F - C) \bmod F$ and the sign of $(b(n) \bmod F - a(n) \bmod F - C) \bmod F$.
25

5 5. A decoder according to any preceding claim, wherein the selector is arranged to select and output the modulo of the linear approximation of a MAX*function if the value $|a(n) - b(n)|$ is less than the predetermined threshold value.

10 6. A decoder according to any preceding claim, wherein the value of F is to the power of two.

7. A decoder according to any preceding claim, wherein the selector is a multiplexer.

15 8. A decoder according to any preceding claim, wherein the calculator is an add module that is arranged to receive $a(n)\text{mod}F$, $b(n)\text{mod}F$ and C.

20 9. A method for generating a MAX* value, the method comprising receiving a first modulo state metric $a(n)\text{mod}F$, a second modulo state metric $b(n)\text{mod}F$ and a predetermined threshold value for $|a(n) - b(n)|$; calculating the modulo of a linear approximation of a MAX* function; and selecting a value from the group $a(n)\text{mod}F$, $b(n)\text{mod}F$, and the calculated modulo based upon a determination as to whether a predetermined threshold value for $|a(n) - b(n)|$ has been met.

25 10. A method according to claim 9, wherein the modulo of the linear approximation of a MAX function is calculated using:
$$\left(a(n)\text{mod}F + \frac{((b(n)\text{mod}F - a(n)\text{mod}F)\text{mod}F + C)}{2} \right) \text{mod}F.$$

5
A method according to claim 9, wherein the modulo of the linear approximation of a MAX function is calculated using:

$$\left(\left(\frac{(a(n) \bmod F + C) \bmod F + b(n) \bmod F}{2} \right) \bmod F + F * s \right) \bmod F, \text{ where } s \text{ is equal to}$$

[$a(m) \bmod F$] and [$((a(m) \bmod F) \bmod F + b(m) \bmod F) \bmod F$].

10

11. A decoder substantially as hereinbefore described with reference to the figures.

15 12. A method substantially as hereinbefore described with reference to the figures.

5 ABSTRACT

A DECODER FOR A WIRELESS COMMUNICATION DEVICE

A decoder for a wireless communication device comprising a calculator for
10 calculating the modulo of a linear approximation of a MAX* function; and a selector
for selecting a MAX* output value from the group $a(n) \bmod F$, $b(n) \bmod F$, and the
calculated modulo based upon a determination as to whether a predetermined
threshold value for $|a(n) - b(n)|$ has been met, where $a(n)$ is a first state metric,
15 $b(n)$ is a second state metric, C is the predetermined threshold value and F is a
value greater than $|a(n) - b(n)|$.

(Figure 4)

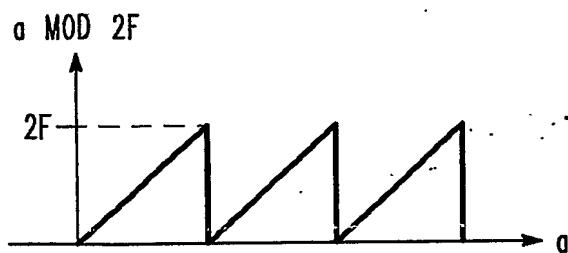


FIG. 1

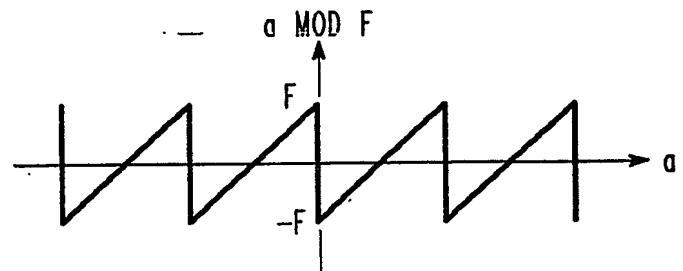


FIG. 2

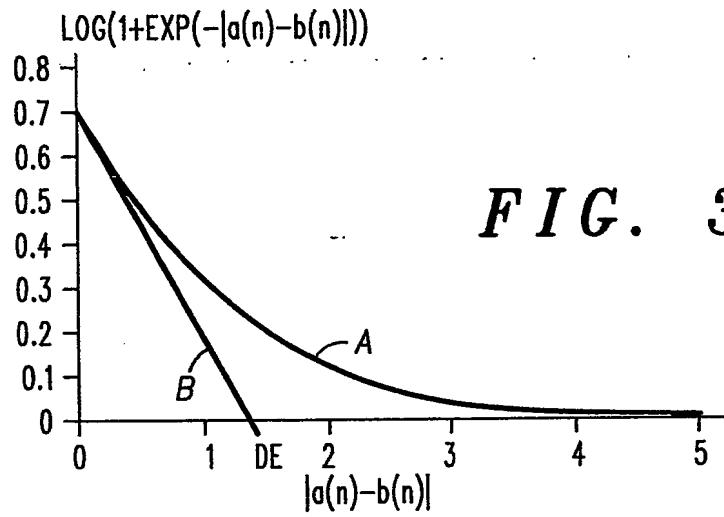
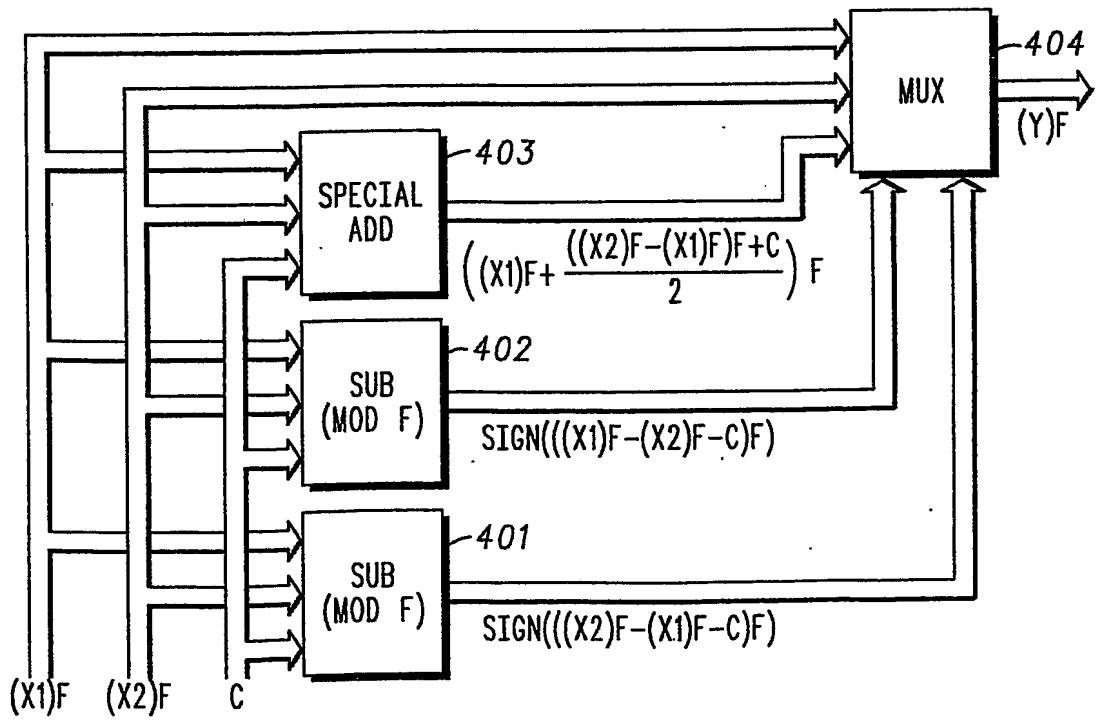


FIG. 3

FIG. 4
400



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